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Microwave Power Harvesting for Satellite Health Monitoring

Alexandru Takacs, *Member, IEEE*, Herve Aubert, *Senior member, IEEE*, Stephane Fredon, Laurent Despoisse, Henri Blondeaux

Abstract—This paper addresses the microwave energy harvesting on board of geostationary satellites for health satellite monitoring. To prove the feasibility of such a concept, we investigated the electromagnetic environment existing on antenna panels. Based on established cartographic maps, three designs of rectennas are proposed. Measured DC powers ranging from 0.256 mW to 1.28 mW can be harvested for electric field levels ranging from 91 V/m to 121 V/m and by using very simple and compact designs. The harvesting structures consist of only one Schottky diode per rectenna and present a total surface of 2.4 cm². They are suitable for powering the new generation of ultra-low power transceivers, thus enabling autonomous wireless power networks for satellite health monitoring.

Index Terms—Energy harvesting, rectennas, satellite applications, microwave circuits, autonomous wireless sensors.

I. INTRODUCTION

HEALTH MONITORING is a key issue for any satellite application and especially for the implementation of reliable and long-life satellite-based broadcasting links. In order to provide reliable and high bit rate broadcasting links, high gain microwave antennas operating in C, X, Ku, K or Ka band are used. These antennas are located on panels positioned on the external surface of the satellite. Surveying the health of these panels involves the use of sensors (e.g. for thermal or for mechanical/structural monitoring) deployed in small networks to cover the targeted surface. A very promising solution is to implement small autonomous wireless sensor networks saving the cost of deploying long wires in harsh environments. In some areas located on antenna panels of broadcasting satellites, the electric field generated by the spill-over loss of microwave antennas can reach the following maximum levels (effective values): 40 V/m in C-band, 49.5 V/m in X-band, 106 V/m in Ku-band and 127 V/m in K-band. These high-frequency electromagnetic field levels are unusual for terrestrial applications, but they are available on satellites if data links are functional and can be harvested in order to

power autonomous wireless sensors used for monitoring the structural health of the satellite. Moreover, the electromagnetic power radiated by microwave antennas is almost constant and consequently the DC power regulatory circuits should be minimal for harvesting systems.

The electromagnetic environment of the antenna panels is analyzed in Section II. Rectenna (RECTifier antENNA) topologies [1] and design methodology developed for proving the concept of microwave power harvesting for satellite health monitoring are discussed in Section III. The main goal of this paper is to demonstrate that microwave energy harvesting based on specific rectenna designs is an ideal solution for powering autonomous sensors for satellite health monitoring.

II. ELECTROMAGNETIC ENVIRONMENT

Broadcasting satellite antennas operating in C, X, Ku and K band radiate electromagnetic power between 50W and 100W with linearly or circularly polarized electromagnetic field. Recently, Thales Alenia Space© performed an analysis of the electromagnetic energy illuminating antenna panels. Intensive electromagnetic simulations using GRASP software from TICRA [2] were performed by taking into account the case of a Spacebus class C satellite. Figs. 1 to 4 show typical electromagnetic field levels (E-field in V/m, peak values) on panels located on the lateral side or on the Earth side of a broadcasting geostationary satellite. These levels were obtained in C, Ku and K frequency bands. We observed that large areas of antenna panels are covered with field levels higher than 4 V/m. This electromagnetic field available at the surface of antenna panels can be advantageously harvested by using rectennas [3] for supplying power to autonomous sensors dedicated to satellite health monitoring. As shown in Fig. 3 a maximum E-field level of 180 V/m (peak value) can be reached at 17.7 GHz.

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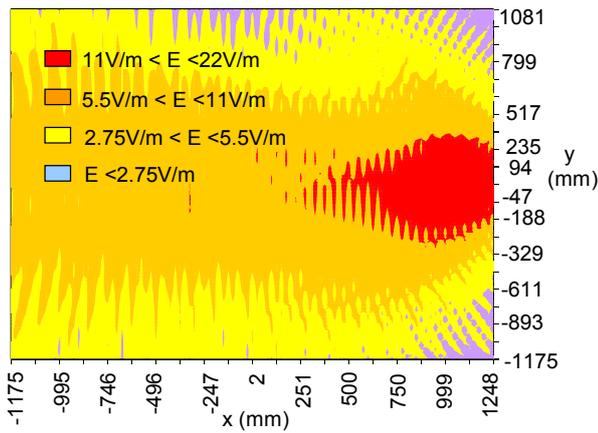


Fig. 1. E-field distribution (peak value) on a lateral panel at 3.5 GHz (C-band). Radiated power: 90 W. The x- and y-coordinates are in millimeter.

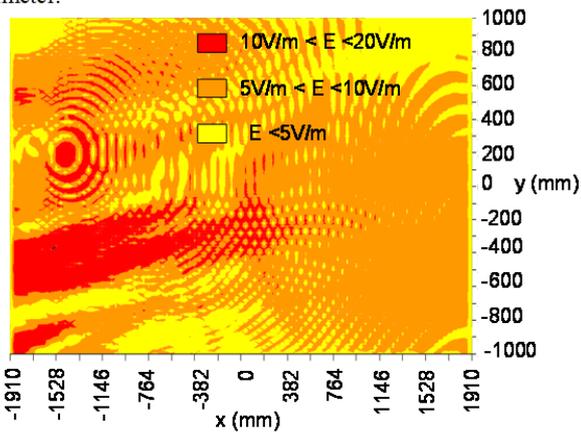


Fig. 2. E-field distribution (peak value) on a lateral panel at 10.7 GHz (Ku-band). Radiated power: 86.5 W. The x- and y-coordinates are in millimeter.

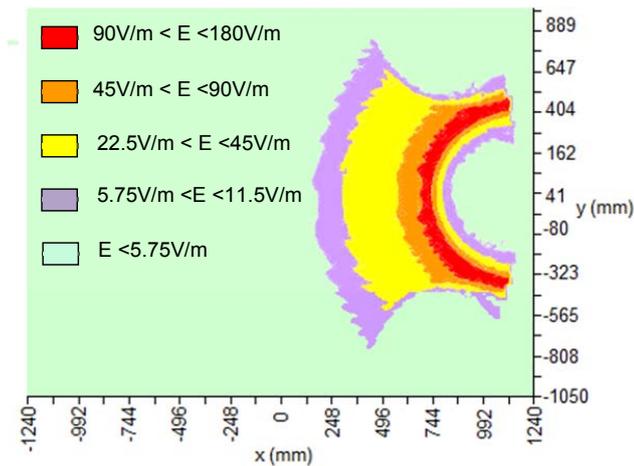


Fig. 3. E-field distribution (peak values) on Earth side of satellite at 17.7 GHz. Radiated power: 70W. The x- and y-coordinates are in millimeter.

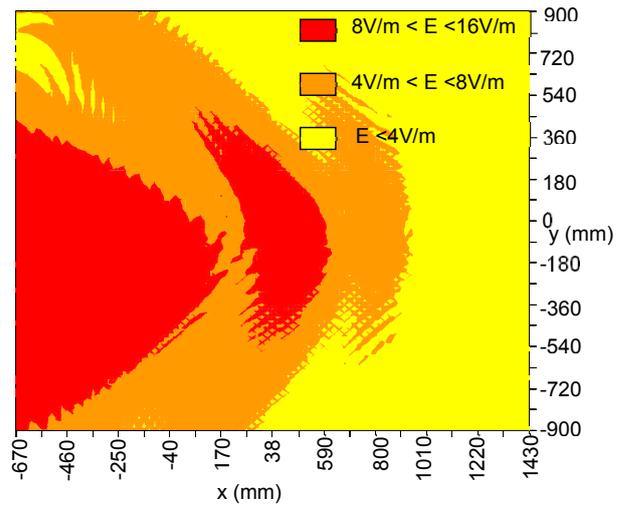


Fig. 4. E-field distribution (peak values) on a lateral side of satellite at 21.4 GHz. Radiated power: 85W and. The x- and y-coordinates are in millimeter.

As shown previously (Fig. 1 to Fig. 4) satellite panels can be illuminated with electromagnetic energy at various frequencies. Moreover the incident waves illuminating satellite panels arrives various directions and have various polarizations (dependently on satellite antennas types and their mounting position). Thus the antenna of the rectenna has to be engineered to meet these criteria (operating frequency, polarization and radiation pattern shape/tilt angle) in order to maximize the amount of the RF power injected at the input of the (rectenna) rectifier.

III. MICROWAVE RECTENNAS: DESIGN AND MEASUREMENT RESULTS

Rectennas are intensively used for wireless power transfer or energy harvesting applications. Many designs and topologies have been proposed for various applications, such as GSM [4], GPS [5], C-band (ISM 2.45 GHz) [6]-[10], 5.8 GHz [10] and X-band [11],[12] applications. Dual-band [9] or broadband [12] designs have been studied while applications beyond 10 GHz have been addressed in the past mainly for wireless power transfer [13] application [3],[14]-[15] but not for power harvesting because of the lack of powerful environmental electromagnetic sources for terrestrial applications. Several research works have been reported on the rectenna design for energy harvesting at frequencies higher than 10 GHz [16]-[19]. A reconfigurable rectenna device that is capable of adapting itself to the incident power level is described in [20]. In order to evaluate the feasibility of such microwave energy harvesting, several rectennas were designed and the measured DC power was compared with typical power requirements for wireless transceivers. Note that ultra-low power receivers are now available [21] and their power consumption is around 2 mW only (voltage supply of 1.2V-1.8V with current below 2 mA).

A. Rectenna topology

In order to keep the proposed designs compatible with the specific technical requirements for space applications, several design guidelines were adopted: (i) the rectenna topology has to be as simple as possible; (ii) all the components in the rectenna (dielectric substrate, diode, capacitors, etc) must be qualified for space applications, ready to be qualified or at least with performances compatible with space requirements; (iii) the operating frequencies must be chosen by taking into account the electromagnetic environment existing on board of satellite antenna panels (typical E-field distributions were presented in Section II) and, (iv) a non-optimal DC loading for rectenna could be chosen, in this a worst case scenario the input impedance/resistance of the sensors and/or the transceiver to be powered may be far from the optimal DC load that maximizes the DC power generated by the rectenna. Keeping in mind these design requirements, the rectenna was designed to power a temperature sensor (load) with a typical resistance in the range of 9-10 k Ω . The rectenna was fabricated on Rogers 6002 substrate (relative permittivity: 2.94, loss tangent: 0.0012, thickness: 508 μm , metallization thickness: 35 μm) [22]. Two GaAs flip chip Schottky diodes were selected: M/A Com MA4E-1317 diode [23] and Aeroflex/Metelics MZBD-9161 diode [24]. These diodes were chosen based on their RF power handling, thermal capabilities and high operating frequency. An important issue in rectenna design is the antenna that should: (i) match the polarization of the incident electromagnetic field, (ii) have a gain as high as possible in order to increase rectenna conversion efficiency, (iii) present a high large half-power beamwidth to efficiently operate for various directions of the incident field and, (iv) be easily matched to the rectifier at the operating frequency. Reproducing in Laboratory the electromagnetic environment existing on satellite panels is not an easy task. As presented in Section III.C, by using the setup S2 an incident wave illuminating the rectenna under test with a linearly polarized E-field, with various power densities (E-field levels) and at various frequencies can be easily generated in Laboratory. Consequently we selected (for our rectennas designs) linearly polarized antennas with at least 50° half-power beam-width and a maximum gain of at least 4 dBi.

The proposed rectenna designs are based on the topology shown in Fig. 5. The antenna collects the surrounding electromagnetic power density and transfers it at the input of the rectifier (Schottky diode) through a matching circuit. The matching circuit allows the conjugate impedance matching and maximizes the RF power level flowing from the antenna to the rectifier. Moreover, the matching circuit should stop the reflected power at the operating frequency and harmonics to be radiated by the antenna. The rectifier converts the RF power to a DC power. The DC power is injected into the load through a low-pass filter that blocks any undesirable RF signal at operating frequency or harmonics. In order to facilitate the testing and debugging of such a rectenna, a 50 Ω test point (end-launch K connector) was added between the antenna and the matching circuit. Although it may introduce undesirable

losses and impedance mismatch, this 50 Ω test point was very useful in the early stages of the design.

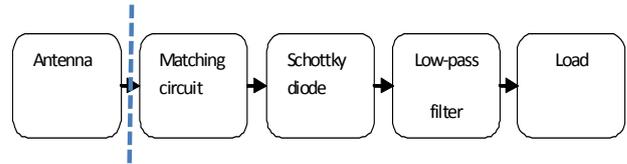


Fig. 5. Rectenna topology: the vertical dotted line indicates the position (reference plane) of the 50 Ω test point (end-launch K connector).

Based on the topology sketched in Fig. 5, three rectennas were designed, fabricated and measured. These rectennas, named R1 (R1a and R1b), R2 (R2a and R2b) and R3 (R3a and R3b), are shown in Fig. 6. The rectennas R1a (using the MA4E-1317 diode) and R1b (using the MZBD-9161 diode) were the first developed demonstrator. Only the rectifier and its 50 Ω input port are shown in Fig. 6. They used only a single stub matching circuit and a lumped RC low-pass filter. The 10k Ω load impedance is integrated in the filter structure. The results obtained with these simple topologies were recently reported by the authors [16]. The main drawback of the R1-rectenna is its low efficiency at 17.7 GHz and consequently a high gain (horn) antenna is needed for harvesting a DC power higher than 2 mW. Two new rectenna designs named R2 and R3 with improved harvesting performances were developed and are now presented.

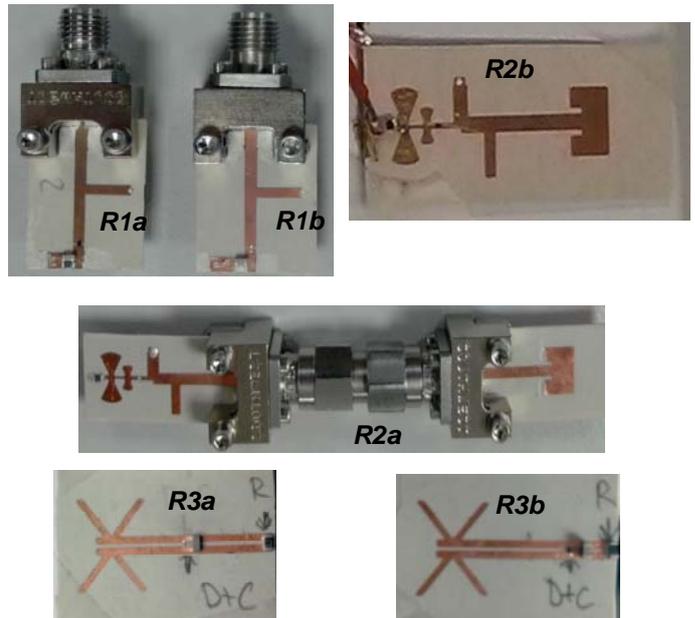


Fig. 6. Photos of the developed rectenna designs: R1 (R1a and R1b), R2 (R2a and R2b) and R3 (R3a and R3b)

The rectenna R2 uses the MA4E-1317 diode, a double stub matching circuit and a distributed low-pass filter containing two radial stubs. The radial stubs were designed for rejecting the operating frequency (17.7 GHz) and the second-order harmonic (35.4 GHz). The rectenna R2a was composed of a rectifier and a patch antenna having a gain around 4 dBi. The rectifier and the antenna are connected using a K-adapter. The

50 Ω test point allows characterizing the rectifier and the antenna performances separately. This test point was eliminated in the rectenna R2b. The rectenna R3 is more compact. A similar topology, based on dual dipole like (DDL) antenna and operating at 2.45 GHz, was proposed in [9]. The antenna was excited by a coplanar stripline. No matching circuit was necessary, and the maximum power transfer (between antenna and diode/rectifier input) and the suppression of the undesirable reflected power at the second harmonic were achieved by properly controlling the input impedance of the antenna. A capacitance of 1.5 pF was used for shunting the RF signal at the operating frequency and its harmonics. In order to maximize the performances of this design, it is crucial to properly control the diode mounting position.

B. Rectennas design and simulation methodology

One of the major challenges in the effective design of rectennas in the microwave frequency range (Ku band and higher) is the accurate non-linear modeling of the diode. The most relevant parameters of the MA4E-1317 diode were derived from an available datasheet [23] (total capacitance: 0.045 pF, series resistance: $R_s=4 \Omega$) and from the extrapolation of the I-V measured characteristic (derived ideality factor: $n\approx 1.2$ and saturation current: $I_s\approx 0.1 \text{ pA}$). For the MZBD-9161 diode, the Spice equivalent model proposed in [24] was used but with a much lower breakdown voltage (3.5 V instead of the 10 V given in the datasheet). A lower breakdown voltage was needed to accurately model the observed nonlinear power behavior of the diode. The simulation model for the MZBD-9161 diode given in [24] uses two anti-parallel diodes (with different parameters) in order to simulate the single Schottky diode used in the rectenna. Fig. 7 shows the complete simulation model in AWR software [25] for the rectenna R2 (without the patch antenna) using closed-form models for the distributed components (transmission lines, stubs and via hole).

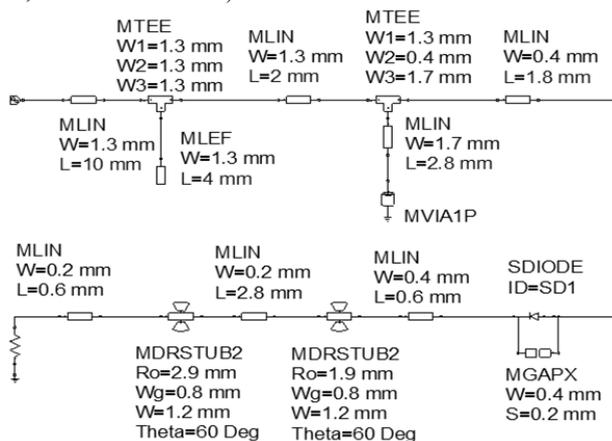


Fig. 7. Simulation model (AWR) of the rectenna R2a (without patch antenna) and its dimensions.

The harmonic balance simulation engine was used for performing non-linear simulations. A generic non-physical

diode model available in AWR software [25] was customized with the MA4E-1317 and MZBD-9161 diode parameters. The rectangular patch antenna was designed, simulated and optimized using the HFSS antenna design kit [26].

The design procedure for the design of the rectenna R3 was quite different. First the DDL antenna was designed and simulated using FEKO [27] for operation at the desired frequency (17.7 GHz). The antenna radiation pattern, gain and radiation efficiency were calculated and the distribution of the electric currents on the metallic strips were analyzed. The design requires a low load resistance for working efficiently. A load of 510 Ω was used. For simulation purposes, the diode was replaced by a voltage port while the capacitance (1.5 pF) and the load (510 Ω) were modeled as port loads. Fig. 8 shows a top view of the rectenna R3. The dimensions of the R3 design are: $l_x=20\text{mm}$, $l_y=14\text{mm}$, $l_d=5.5\text{mm}$, $l_r=15\text{mm}$, $l_s=1.4\text{mm}$, $l_{ax}=6.3\text{mm}$ and $l_{ay}=8.3\text{mm}$. The coplanar strip line is characterized by a strip width of $w=0.8 \text{ mm}$ and a gap size of $g=0.4 \text{ mm}$. A metallic plate (dotted line contour in the Fig. 8) was printed below the radiating element ($l_{gx}=10\text{mm}$ and $l_y=14\text{mm}$). R3 design is very compact with a total surface of 2.4 cm².

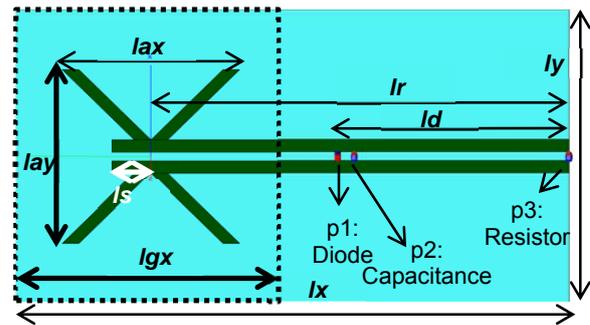


Fig. 8. Simulation model (Feko) of the R3-rectenna design (see the text for the dimensions)

C. Experimental setup

Two experimental setup configurations, named S1 and S2, were used. In the S1 setup shown in Fig. 9 a continuous millimeter-wave signal generated from an Anritsu MG3694B generator was directly injected at the 50 Ω test point of the manufactured prototypes and the resulting DC voltage was measured at the input port of the load impedance with a Keythley 2000 multimeter.

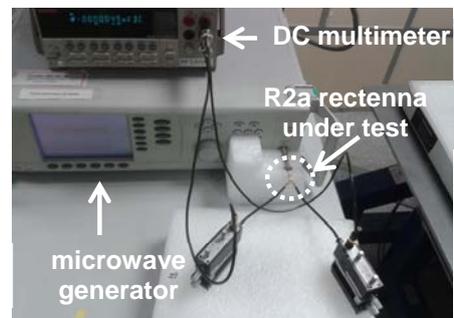


Fig. 9. Setup S1.

The setup (S1) is appropriate for testing the rectifier part

(e.g. R1a, R1b, R2a) of the rectennas when equipped with a 50Ω test point (coaxial K connector). In the S2 setup shown in Fig. 10, a microwave signal generated from an Anritsu MG3694B generator was injected at the input of a horn antenna (VT220HA20-SK from Vector Telecom [28]) which illuminated the rectenna under test with a linear polarized E-field. This setup is appropriate for testing the rectennas (R2b, R3) or rectifiers equipped with a 50Ω test point/coaxial K connector (e.g. R1a, R1b, R2a) connected with an external antenna.

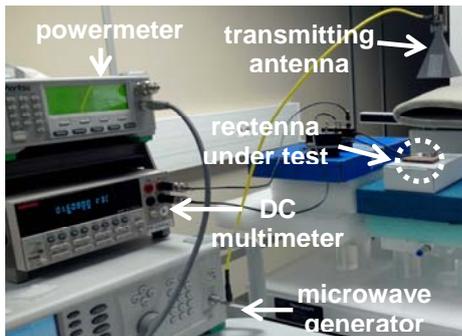


Fig. 10. Setup S2.

An automatic acquisition routine was implemented in Labview software from National Instruments [29] in order to speed-up the acquisition process. The harvested DC voltage was measured with the microwave source OFF (DC noise: V_{off}) and with microwave source ON (DC voltage: V_{on}). The DC voltage of interest (V_{out}) was then derived from the difference $V_{out} = V_{on} - V_{off}$. Digital filters were used for minimizing the noise level. The measurement was performed twice and the average value of V_{out} was registered as the final result.

D. Simulation and experimental results

The layouts of rectennas were accommodated with the tolerances required by a fabrication in a laboratory equipped for general-purpose printed circuit boards (PCB). A solid silver-filled epoxy system EPO-TEK@H20E was used for soldering the diodes by a low temperature process (110°C).

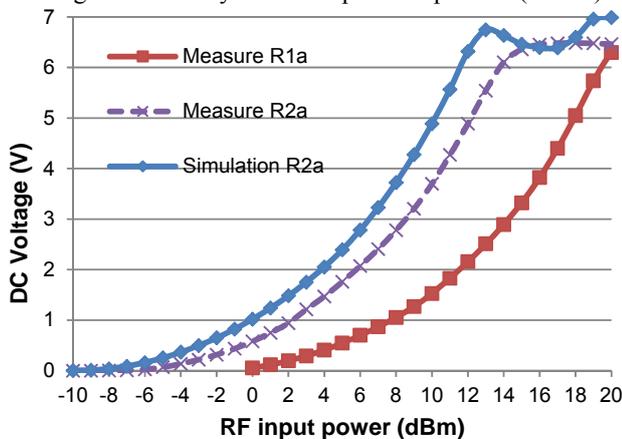


Fig. 11. Measured DC output voltages (setup S1) for R1a (dotted red line, square marker) and R2a (dotted violet line, 'x' marker design).

The simulation results obtained by using AWR simulation model for R2a are represented with a continuous (blue) line (diamond marker).

Fig. 11 and Fig. 12 show a comparison between the measured performances (by using the setup S1) of the rectifiers R1a and R2a in terms of the harvested DC voltage (Fig. 11) and DC power (Fig. 12) at the input of the load impedance ($10\text{ k}\Omega$).

A DC voltage up to 6.4 V and a DC power up to 4 mW can be harvested with the R2a design when a RF power around 15 dBm is injected at the input of the rectifier (Schottky diode). A maximum worst-case efficiency of 15.4% was achieved for a RF input power of 13 dBm (experimental results). This worst case efficiency takes into account the losses and the impedance mismatch introduced by the 50Ω K-connector and by the male-to-male K-adapter. This low efficiency is mainly due to the non-optimal load impedance ($10\text{ k}\Omega$) chosen as reference.

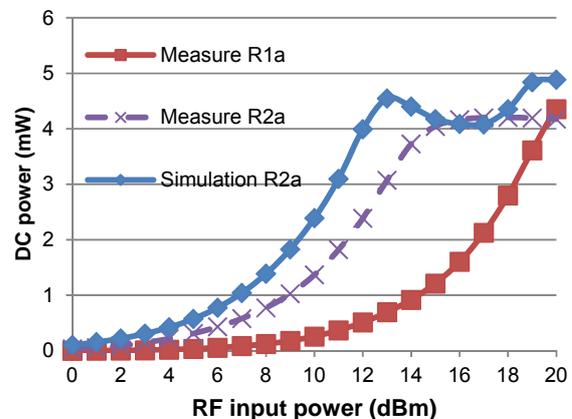


Fig. 12. Measured DC output power (setup S1) for R1a (dotted red line, square marker) and R2a (dotted violet line, 'x' marker design). The simulation results obtained by using AWR simulation model for R2a are represented with a continuous (blue) line (diamond marker).

Precursory of the R1a/R1b structures, reported in [30]-[31] were tested in CNES (French Space Agency) Laboratory by applying a standard thermal cycling procedure for space applications (30 thermal cycles performed between -65°C and $+125^\circ\text{C}$). Despite of the *soldering-free* home-made fixation system the prototypes still remained operational after the thermal cycling without a major impact on the RF performances.

The output DC voltage as a function of the operating frequency obtained for a RF input power of 13 dBm is displayed in the Fig. 13. The maximum voltage of 5.4 V was obtained at 17.7 GHz , which is the central operating frequency of the single stub matching circuit.

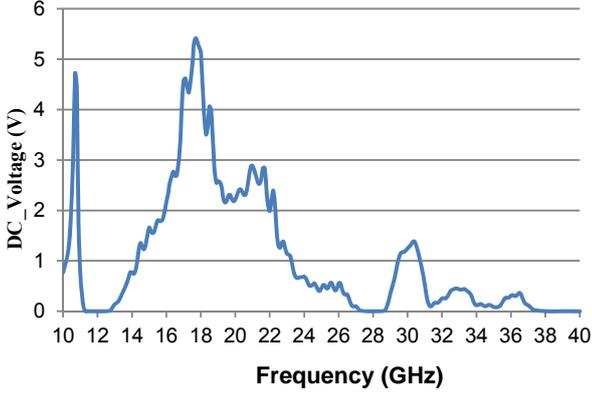


Fig. 13. Measured DC output voltage (setup S1) for R2a design as a function of the frequency for an RF power of 13 dBm at the input of 50Ω test point.

Fig. 14 shows the measured DC voltage harvested by the R2b-rectenna design when illuminated with the electric field of a horn antenna (gain: 18.6 dBi at 17.7 GHz). A microwave power ranging from 10 to 24 dBm was injected at the input of the horn antenna. The distance between the radiating aperture of the horn antenna and the rectenna R2b is 15 cm. The input port (coaxial K connector) of the transmitting horn antenna is located at 25 cm above the rectenna R2b under test. A maximum DC voltage of 1.6 V was measured and a low harvested DC power of 0.256 mW was obtained. In order to measure the RF power collected by the patch antenna, a calibrated Anritsu ML2437A powermeter was used. The measured RF power received with the patch antenna alone (gain: 5dBi at 17.7GHz) was found to be 4.5dBm: when this RF power was directly injected at the input port of the rectifier (using the 50Ω test point of R2a in the setup S1), the harvested DC voltage was found to be 1.63 V. Consequently, the measurement results obtained using setup S2 (Fig. 14) are coherent with the results depicted in Fig. 11.

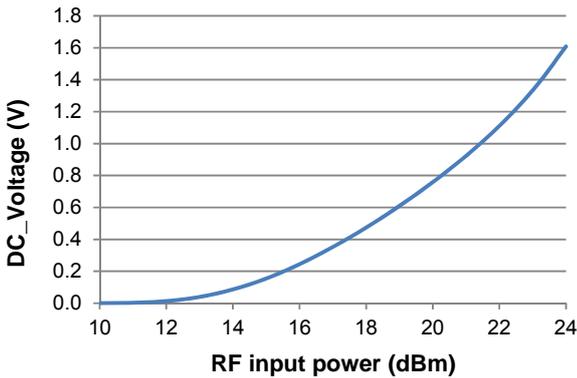


Fig. 14. Measured DC output voltage (setup S2) for the R2b-rectenna design as a function of the RF power injected at the input port of a transmitting (horn) antenna (operating frequency: 17.7 GHz).

To obtain a harvested DC power higher than 2mW, an antenna with a gain of at least 12dBi should be used instead of the patch antenna. Alternatively a DC combining circuit could

be proposed to combine the DC power harvested from many rectennas [1].

The power P received at a given frequency by an antenna of gain G at a location where an electric field level E exists can be approximated by [32]:

$$P = \frac{E^2}{120 \cdot \pi} \cdot \frac{G \cdot \lambda^2}{4 \cdot \pi} \quad (1)$$

where λ denotes the free-space wavelength. Consequently, the RF power at the output of the receiving antenna (input of the 50Ω test point) can be estimated for a given incident E-field level (table 1). Eq. (1) can be also written as:

$$E = \frac{2 \cdot \pi}{\lambda} \cdot \sqrt{\frac{120 \cdot P}{G}} \quad (2)$$

When specifying the required RF power at the output of a calibrated antenna (with a known gain), the needed E-field level can then be derived from Eq.(2). Three typical antenna gains were considered: 18.6 dBi (e.g. horn antenna), 11 dBi (for comparison purposes) and 5 dBi (e.g. patch antenna).

Table 1: Estimated RF power at the input of the 50Ω test point, measured DC voltage extracted from Fig.11 and the computed DC power for R2a design ($f=17.7\text{GHz}$)

E (V/m)	G (dBi)	RF power (dBm)	R2a design (MA4E-1317)	
			DC voltage (V)	DC power (mW)
107	18.6	17	6.48	4.2
67	18.6	13	5.54	3.07
48	18.6	10	3.67	1.37
34	18.6	8	2.78	0.77
27	18.6	5	1.75	0.31
15	18.6	0	0.58	0.033
127	11	10.9	4.27	1.82
91	11	8	2.78	0.77
72	11	6	2.07	0.43
51	11	3	1.21	0.015
36	11	0	0.58	0.033
127	5	4.9	1.75	0.31
121	5	4.5	1.6	0.28
114.5	5	4	1.47	0.21
102	5	3	1.21	0.015
91	5	2	0.94	0.088
72	5	0	0.58	0.033

To design rectenna R3, the variation of the input impedance of DDL antenna as a function of the diode mounting position was analyzed. The simulated input impedance Z_{in} of the antenna viewed at the distance l_r-l_d along the coplanar stripline is depicted in Fig. 15 as a function of l_d (see Fig. 7). The imaginary part (reactance) was found to be positive. As the estimated input impedance of the MZBD-9161 diode is $8 - j*80 \Omega$ the diode should be located approximately at $l_d=5.5$ mm to ensure the conjugate impedance matching condition. Moreover since the (simulated) impedance Z_{in} at $l_d=5.5$ mm is $24.5+j*130 \Omega$ at 35.4 GHz (i.e., at the first harmonics) and

$204+j*203 \Omega$ at 53.1 GHz (i.e., at the second harmonics), the reflected power radiated back by the antenna of the rectenna (R3 design) is expected to be small at the first two higher-order harmonics.

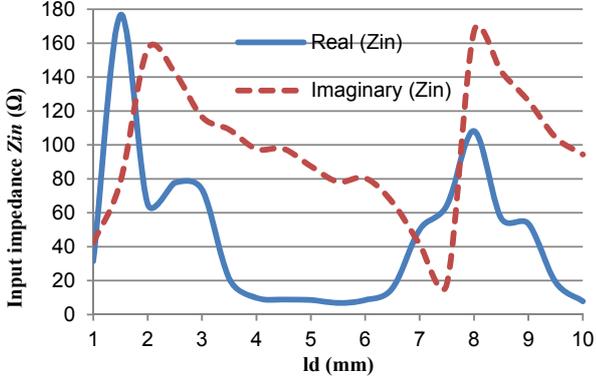


Fig. 15. Simulated input impedance Z_{in} of the antenna (R3 design) viewed at the distance l_r-l_d along the coplanar stripline as a function of l_d .

The simulated radiation pattern displayed in Fig. 16 shows that the maximum gain of the DDL antenna is approximately 6 dBi.

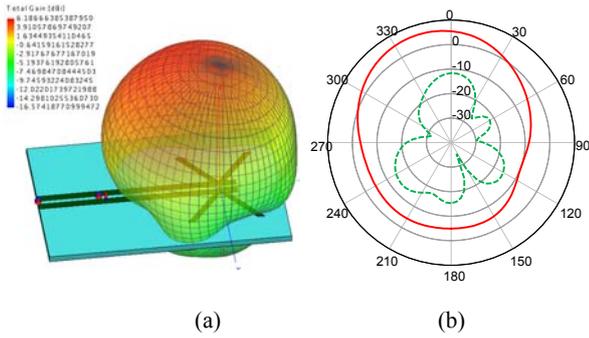


Fig. 16. Simulated radiation pattern (gain) of rectenna R3a: a) 3D radiation pattern and b) E-plane polar cut: main (E_{ϕ}) and cross (E_{θ}) components of the total gain (values in dB, angles in degrees) are represented with continuous (red) and dotted (green) lines, respectively.

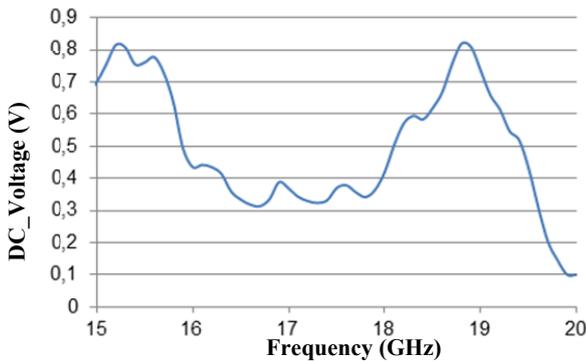


Fig. 17. Measured DC voltage (S2 setup) at the input of the load (510Ω) as a function of the frequency (R3 design).

The measured DC voltage (setup S2, power injected at the input of a horn antenna: 23 dBm, distance between the horn aperture and the R3a rectenna: $d=15$ cm) as a function of the frequency is depicted in Fig. 17.

A maximum DC voltage of 0.81 V (DC power of 1.28 mW) was recorded at a frequency of 18.8 GHz while a DC voltage of only 0.36 V (DC power of 0.25 mW) is measured at the targeted operating frequency $f=17.7$ GHz. This can be explained by: (i) the inaccuracy of the adopted design methodology (in the electromagnetic model the antenna is loaded by a voltage electromagnetic port instead of the actual nonlinear loading of the diode); (ii) manufacturing tolerances (all the rectennas were fabricated in an university laboratory not equipped for high-frequency PCB manufacturing); (iii) error in the positioning of the diode during its mounting on the PCB. However the rectenna R3a is very compact (2.8 cm^2) and performs very well in a very wide frequency range (from 15 to 20 GHz). The measured RF power (using a calibrated Anritsu ML2437A powermeter) at the output of manufactured patch antenna is 2dBm and is consistent with the E-field level of 91 V/m at 17.7 GHz estimated on the rectenna surface. In order to calculate the efficiency η (in %) of this rectenna the following worst case definition is used [7], [33]:

$$\eta = \frac{P_{DC}}{S \cdot A_G} \cdot 100 \quad (3)$$

where P_{DC} is the measured harvested DC power, S is the incident power density and A_G denotes the area of the radiating surface. The power density (expressed in $\mu\text{W}/\text{cm}^2$) can be computed as function of E-field effective value E on the antenna surface as follows:

$$S = \frac{E^2}{120 \cdot \pi} \cdot 100 \quad (4)$$

In the case of the R3 design an efficiency of 42% is derived for $A_G=1.4 \text{ cm}^2$ and $E=91 \text{ V/m}$ (we consider here that the geometrical surface of antenna is the surface of the metallic plate printed below the DDL radiating element, that is $10\text{mm} \times 14\text{mm}$). Taking into account the geometrical surface of the patch antenna which is approximately 1 cm^2 for the rectenna R2b we obtain a worst-case efficiency of 11.4 % ($A_G=1 \text{ cm}^2$ and $E=91 \text{ V/m}$) according to eq. 3. This low efficiency can be explained by: (i) the non-optimal loading of the MA4E-1317 diode by a $10 \text{ k}\Omega$ load and (ii) the MA4E-1317 diode (forward voltage in the range of 0.7 V) serially connected with the patch antenna requires a high RF input power in order to be properly self-biased and to operate efficiently. This high RF input power cannot be delivered by the patch antenna under the test condition (setup S2, incident E-field : $E=91 \text{ V/m}$).

Several rectennas operating at frequencies beyond 10 GHz were reported in the literature [14]-[19]. Table 2 summarizes the performances (efficiency: eff in % as function of the frequency: f in GHz and size in mm^2) of these rectennas compared with our work. We note that only the references [14]-[15] present measured values (with a setup and

experimental conditions well detailed) for the overall efficiency of the rectennas.

Table 2: Comparison of the rectennas performances for reported design (beyond of 10 GHz).

eff (%)	f (GHz)	Diode	Size (mm ²)	Note
39	35	DMK6606 (Alpha)	>24	[14]: a waveguide array simulation technique [34] was used to measure the overall rectenna efficiency; the reported efficiency defined as the ratio of DC power to the input power into diode was measured for 60 mW of input power into the diode and for an optimum load of 400Ω
35	35	M/A Com MA4E-1317	>110	[15]: the reported efficiency (received RF power/output DC power) was measured using a free space setup for an incident power density of 30 mW/cm ² and for a load resistance of 50Ω
54.6	24	M/A Com MADS-001317-1320AG	NR*	[16]: the efficiency was measured by illuminating the rectenna with a signal delivered by a waveguide expander positioned in the close vicinity of the rectenna under test. The reported value was obtained for 130 mW of RF input power (supposed to be at the input of the rectifier) and an optimal load of 400 Ω
82	24	M/A Com MA4E-1317	NR*	[17]: the reported efficiency (for 5 mW of RF power at the input of the rectifier) concerns only the microwave rectifier loaded by an optimal resistive load (value NR*)
17	25.7	M/A Com MA4E-2502L	328.5	[19]: only the efficiency of the rectifier part is reported; value obtained for a RF power of 8 dBm at the input of the diode and an optimal load of 1500 Ω
42	18.8	Metelics MZBD-9161	280	This paper: the rectenna efficiency (worst case definition: eq. 3) was measured by using the setup S2, for an incident E-field of 91 V/m (incident power density around of 2.2 mW/cm ²) and for a load of 510 Ω

*NR: Not Reported

We note that for lower frequencies (e.g. 2.45 GHz or below) higher efficiencies (up to 80%) can be obtained.

IV. CONCLUSION

We present the cartography of the electromagnetic environment available on antenna panels of broadcasting geostationary satellites. Large areas of those panels are illuminated with an electromagnetic field ranging from 4 V/m to 127 V/m. This electromagnetic energy can be harvested to supply power to wireless sensor networks for satellite health monitoring. In order to prove the feasibility of the concept three rectennas, named R1, R2 and R3, were proposed. The rectennas were developed in a worst case scenario, namely when the rectifier/Schottky diode is not optimally loaded by the DC load impedance. Moreover, constraints concerning the space applications were taken into account in the rectennas design. Measured DC powers ranging from 0.256 mW (R2 design for an incident E-field level around 121 V/m) to 1.28

mW (R3 design for an incident E-field around 91 V/m) were harvested. If a higher antenna gain is used in the R2 design, a DC power higher than 2 mW, (i.e. the typical power consumption of the new generation of ultra-low power transceivers) may be harvested. The very compact rectenna (design R3 with a total surface of 2.8 cm²) can harvest a DC power around 2 mW if more electromagnetic energy is available (e.g. if the E-field level reaches 127 V/m). Moreover, the well-known stability of the microwave links will reduce the complexity of any DC power management, storage, or regulatory circuits.

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